

## Nonreciprocal and Non-Hermitian Material Response Inspired by Semiconductor Transistors

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Here, inspired by the operation of conventional semiconductor transistors, we introduce a novel class of bulk materials with nonreciprocal and non-Hermitian electromagnetic response. Our analysis shows that material nonlinearities combined with a static electric bias may lead to a *linearized* permittivity tensor that lacks the Hermitian and transpose symmetries. Remarkably, the material can either dissipate or generate energy, depending on the relative phase of the electric field components. We introduce a simple design for an electromagnetic isolator based on an idealized “MOSFET-metamaterial” and show that its performance can in principle surpass conventional Faraday isolators due to the material gain. Furthermore, it is suggested that analogous material responses may be engineered in natural media in nonequilibrium situations. Our solution determines an entirely novel paradigm to break the electromagnetic reciprocity in a bulk nonlinear material using a static electric bias.

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The Lorentz reciprocity law constrains the propagation of electromagnetic waves in conventional photonic platforms [1,2]. For Hermitian systems, the Lorentz reciprocity is rooted in the linearity of Maxwell's equations and on their invariance under a time-reversal (TR) operation [3]. Generically, a nonreciprocal electromagnetic response requires either (i) breaking the TR symmetry with a suitable bias, or (ii) using nonlinear materials, or (iii) exploiting non-Hermitian physics.

The standard solution to break reciprocity is by using a static magnetic field bias. The magnetic field is odd under the TR operation and thereby may give rise to a gyrotropic nonreciprocal permeability in ferrimagnetic materials [1,4] or a gyroelectric nonreciprocal permittivity in magnetized plasmas [5,6]. Such material platforms are extensively used to realize optical isolators and circulators [4,7], and due to their topological properties [8] may enable “one-way” propagation free of backscattering [9–20]. However, the necessity of an external magnetic field is a major drawback for the integration of such components on a chip. Alternative magnetless solutions have been investigated in recent years. Such solutions can be subdivided into two classes, depending if they preserve or not the linearity of Maxwell's equations.

For the first class, the material response is linear under normal conditions of operation. Such solutions include time-variant systems [21–35], systems with moving parts [36–38], systems with drifting electrons [39–47], and non-Hermitian platforms, e.g.,  $\mathcal{PT}$ -symmetric systems [48–50], active electronic systems [51–53], or optically pumped systems [54]. It is relevant to point out that time

modulations, the drift current bias, or the velocity bias, all imply an explicitly broken TR symmetry. In contrast, as highlighted recently in Ref. [54], a non-Hermitian response can be compatible with the TR symmetry, but yet break the reciprocity. All the solutions in this first class require some external bias of the system.

The second class is formed by systems that exploit *dynamic* nonlinear effects and that have been implemented in photonic crystals [55–65] or using Fano resonances [66–69],  $\mathcal{PT}$  symmetry [70–72], or other mechanisms [73–77]. These systems are typically self-biased by the incoming wave. Thus, they require input signals with very large power, and generally speaking they cannot provide a robust optical isolation [77–79].

Here, inspired by the physics of transistors, we unveil a different opportunity to generate a strongly nonreciprocal and non-Hermitian *linearized* material response, which relies on the combination of a static electric bias with nonlinearities. Crucially, even though the material nonlinearity is essential to break the reciprocity, in our system the effective material response to weak dynamical signals can be assumed linear. This property may be understood with an analogy with semiconductor transistors, which are nonlinear devices biased by static fields, and then behave as linear systems (e.g., amplifiers) for relatively weak dynamical signals.

It is curious to note that the nonreciprocal responses of other well-known systems with a broken TR symmetry also rely on nonlinear effects that are linearized around a biasing point for small amplitude signals. For example, the gyrotropic permeability of ferrimagnetic materials and the

gyroelectric permittivity of magnetized plasmas result from the linearization of the magnetic torque and of the Lorentz force, respectively [1]. Similarly, the nonreciprocal response of materials with a drift current results from the linearization of the Boltzmann equation [5,6,80–82]. Furthermore, the linearization of optomechanical interactions is at the origin of the nonreciprocity reported in Refs. [24,83,84].

Here, inspired by this feature and by the operation of standard transistors, we propose a new paradigm to obtain a nonreciprocal linearized response in a bulk nonlinear material, which combines the benefits of the linearized systems cited above with the simplicity of the electric field bias, providing a unique platform for the study of non-Hermitian and nonreciprocal wave phenomena.

As a starting point, consider a standard MOSFET transistor, as depicted in Fig. 1(a)(i). In a MOSFET, the voltage applied on the gate controls the height of the channel that connects the drain and the source [1,85]. Thus, the electric field along the  $z$  direction controls the “polarizability” of the system along the  $x$  direction. Let us imagine a metamaterial formed by many structural unities identical to the MOSFET organized in a lattice [Fig. 1(a)(ii)]. Hereafter we refer to this medium as the MOSFET-metamaterial. We note that metamaterials loaded with transistors have been discussed in seminal works by Caloz and others [51–53] in a different context.

The material constitutive relation that mimics the response of a MOSFET transistor is of the form  $\mathbf{P} = \varepsilon_0 \bar{\chi}(\mathbf{E}) \cdot \mathbf{E}$  with

$$\bar{\chi}(\mathbf{E}) = \begin{pmatrix} \chi_{xx}(E_z) & 0 & 0 \\ 0 & \chi_{yy} & 0 \\ 0 & 0 & \chi_{zz} \end{pmatrix}. \quad (1)$$

Here,  $\mathbf{P}$  is the polarization vector in the metamaterial and  $\mathbf{E}$  is the electric field. The susceptibility  $\chi_{xx}(E_z)$  depends on the field strength along  $z$ , in the same manner as the MOSFET impedance along the drain-to-source channel ( $x$  direction) depends on the gate voltage ( $z$  component of the electric field). Thus, the metamaterial is nonlinear. The polarizabilities  $\chi_{yy}$  and  $\chi_{zz}$  are assumed independent of the field strength. For simplicity we neglect material dispersion so that the susceptibility is frequency independent and real-valued. The dispersive effects could be modeled by noting

that the material response is determined by a set of nonlinear differential equations, which could be linearized using a procedure analogous to what is described below. The main impact of material dispersion is that it usually determines a frequency cutoff beyond which the nonlinear response becomes too weak, and, in addition, the permittivity components may become complex-valued.

Let us suppose that such hypothetical metamaterial is biased with some static electric field in the  $xoz$  plane  $\mathbf{E}_0 = E_{0x}\hat{\mathbf{x}} + E_{0z}\hat{\mathbf{z}}$ . For small field variations ( $\delta\mathbf{E}$ ) around the biasing point ( $\mathbf{E} = \mathbf{E}_0 + \delta\mathbf{E}$ ) the electric response can be linearized as

$$\mathbf{P} \approx \varepsilon_0 \bar{\chi}(\mathbf{E}_0) \cdot \mathbf{E}_0 + \varepsilon_0 \sum_{i=x,y,z} \partial_{E_i} [\bar{\chi}(\mathbf{E}) \cdot \mathbf{E}]|_{\mathbf{E}=\mathbf{E}_0} \delta E_i. \quad (2)$$

In the above,  $\partial_{E_i} \equiv \partial/\partial E_i$  with  $i = x, y, z$ , represents a derivative with respect to the electric field. The induced polarization is  $\mathbf{P} = \mathbf{P}_0 + \delta\mathbf{P}$ , with  $\delta\mathbf{P} = \varepsilon_0 \sum_{i=x,y,z} \partial_{E_i} [\bar{\chi}(\mathbf{E}) \cdot \mathbf{E}]|_{\mathbf{E}=\mathbf{E}_0} \delta E_i$  the linearized signal response. Thus, for sufficiently weak signals, the dynamical parts of the polarization and electric field vectors are related through a linear relation of the form  $\delta\mathbf{P} = \varepsilon_0 \bar{\chi}_{\text{lin}} \cdot \delta\mathbf{E}$  where  $\bar{\chi}_{\text{lin}}$  is the effective (linearized) material susceptibility. It can be written explicitly as

$$\bar{\chi}_{\text{lin}} = \sum_{i=x,y,z} \partial_{E_i} [\bar{\chi}(\mathbf{E}) \cdot \mathbf{E}]|_{\mathbf{E}=\mathbf{E}_0} \otimes \hat{\mathbf{u}}_i, \quad (3)$$

with  $\hat{\mathbf{u}}_i$  a unit vector directed along the  $i$ th direction, and  $\otimes$  represents the tensor product of two vectors. For the particular model in Eq. (1), one finds that

$$\bar{\chi}_{\text{lin}} = \begin{pmatrix} \chi_{xx}(E_{0z}) & 0 & \partial_{E_z} \chi_{xx}|_{\mathbf{E}=\mathbf{E}_0} E_{0x} \\ 0 & \chi_{yy} & 0 \\ 0 & 0 & \chi_{zz} \end{pmatrix}. \quad (4)$$

In general, the linearized response is nonreciprocal because  $\bar{\chi}_{\text{lin}} \neq \bar{\chi}_{\text{lin}}^T$  (the superscript  $T$  represents the matrix transpose). Thus, our proposal establishes a novel paradigm to have nonreciprocity with an electric bias. A nonreciprocal response requires that the bias static field has an  $x$  component ( $E_{0x} \neq 0$ ), i.e., a component along the drain-to-

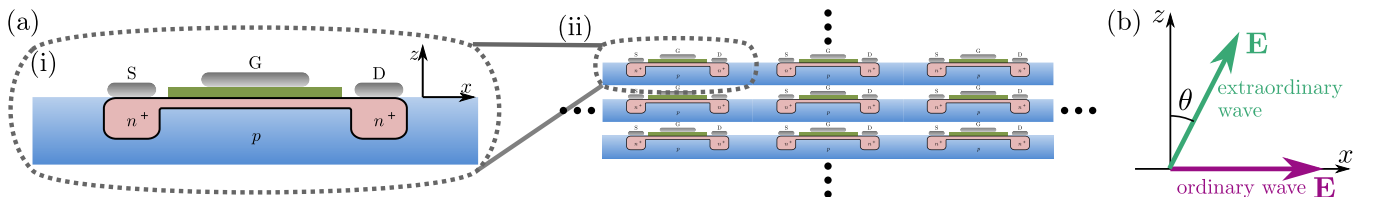


FIG. 1. (a)(i) Sketch of a MOSFET transistor. (ii) Illustration of a metamaterial formed by a periodic array of MOSFETs. (b) Geometrical relation between the  $\mathbf{E}$  field of the plane wave modes in the MOSFET-metamaterial [Eq. (5)] for propagation along  $y$ .

source direction in the MOSFET transistor analogue. The field component  $E_{0z}$  may be zero when  $\partial_{E_z} \chi_{xx}|_{E_z=0} \neq 0$ .

It is rather curious that the microscopic susceptibility is a symmetric tensor [Eq. (1)], but the linearized susceptibility [Eq. (4)] is not. Furthermore, for the considered model, the linearization preserves the TR symmetry of the system. We note in passing that Ref. [54] studied related (but not equivalent) non-Hermitian material responses obtained using optical pumping. In general, a non-Hermitian material response must be rooted in some nonequilibrium process that can extract energy from either the stored electrostatic field or from the DC generator. The latter case is feasible with a drift current, analogous to a MOSFET transistor. Note that in our scheme the drift velocity can be a tiny fraction of the wave velocity, different from other solutions studied previously that rely on materials with large mobility [39–47].

Even though our starting point was an analogy with transistors, related nonreciprocal responses can in principle be engineered using naturally available nonlinear materials. For example, related nonlinearities may naturally occur in crystals without inversion symmetry [86] and may also be engineered in semiconductor superlattices [87]. It is however essential that the material is operated in nonequilibrium (e.g., with carrier injection), as in equilibrium the Kleinman symmetry forces the linearized response to be reciprocal [88,89].

Since the electric displacement vector is  $\mathbf{D} = \epsilon_0 \mathbf{E} + \mathbf{P}$ , the linearized relative permittivity of the metamaterial is  $\bar{\epsilon} = \mathbf{1}_{3 \times 3} + \bar{\chi}_{\text{lin}}$ . Thus, for a MOSFET-metamaterial the permittivity tensor is of the form

$$\bar{\epsilon} = \begin{pmatrix} \epsilon_{xx} & 0 & \epsilon_{xz} \\ 0 & \epsilon_{yy} & 0 \\ 0 & 0 & \epsilon_{zz} \end{pmatrix}. \quad (5)$$

This formula confirms that when the permittivity tensor is real valued and frequency independent, the linearized response remains TR invariant ( $\bar{\epsilon}^* = \bar{\epsilon}$ ), even though it is nonreciprocal ( $\bar{\epsilon}^T \neq \bar{\epsilon}$ ) [90]. Furthermore, the metamaterial is non-Hermitian ( $\bar{\epsilon}^\dagger \neq \bar{\epsilon}$ ), which indicates that it can either absorb or generate energy.

For simplicity, in the remainder of this Letter, we focus on the material response of the idealized MOSFET-metamaterial (5). We are interested only in weak signals described by the linearized response, and thus hereafter, to keep the notations short, we drop the  $\delta$  symbol ( $\delta \mathbf{E} \rightarrow \mathbf{E}$ ), and denote the dynamic electric field simply by  $\mathbf{E}$ .

Next, we characterize the plane wave modes in the metamaterial. The wave equation is of the form  $\nabla \times \nabla \times \mathbf{E} = (\omega^2/c^2) \bar{\epsilon} \cdot \mathbf{E}$ , where  $\omega$  is the angular frequency and  $c$  the speed of light in vacuum. Plane wave solutions are of the form  $\mathbf{E} = \mathbf{A}_0 e^{i\mathbf{k} \cdot \mathbf{r}}$  with  $\mathbf{A}_0$  a constant complex vector,  $\mathbf{k}$  the wave vector and  $\mathbf{r} = x\hat{\mathbf{x}} + y\hat{\mathbf{y}} + z\hat{\mathbf{z}}$  the position vector.

We restrict our attention to propagation along the  $y$  direction, i.e., the direction perpendicular to the gate-drain-source plane [see Fig. 1(a)], so that  $\mathbf{k} = k\hat{\mathbf{y}}$ . In this case, the solutions of the homogeneous wave equation are such that

$$\mathbf{k} = \frac{\omega}{c} \sqrt{\epsilon_{xx}} \hat{\mathbf{y}} \equiv \mathbf{k}_o, \quad \mathbf{E} \sim \hat{\mathbf{x}} \quad (\text{ordinary wave}) \quad (6a)$$

$$\mathbf{k} = \frac{\omega}{c} \sqrt{\epsilon_{zz}} \hat{\mathbf{y}} \equiv \mathbf{k}_e, \\ \mathbf{E} \sim \frac{\epsilon_{xz}}{\epsilon_{zz} - \epsilon_{xx}} \hat{\mathbf{x}} + \hat{\mathbf{z}} \quad (\text{extraordinary wave}). \quad (6b)$$

Remarkably, due to the non-Hermitian response for a nonzero cross-coupling coefficient  $\epsilon_{xz}$ , the ordinary and extraordinary waves are not orthogonal [54,91]. The tilt of the extraordinary wave electric field with respect to the direction perpendicular to the ordinary wave electric field is determined by an angle  $\theta$  such that  $\tan(\theta) = \epsilon_{xz}/(\epsilon_{zz} - \epsilon_{xx})$  [see Fig. 1(b)]. Interestingly,  $\theta$  determines the strength of the nonreciprocal effects. It may differ significantly from zero even for a small cross-coupling coefficient  $\epsilon_{xz}$  provided the values of  $\epsilon_{xx}$  and  $\epsilon_{zz}$  are sufficiently close. The limiting case  $\epsilon_{xx} = \epsilon_{zz}$  corresponds to an exceptional point where the two waves (6) coalesce into a single linear polarization [54] and will not be further considered here.

Consider a superposition of ordinary and extraordinary waves propagating along  $+y$ :

$$\mathbf{E} = A_o e^{ik_o y} \hat{\mathbf{x}} + A_e \left( \frac{\epsilon_{xz}}{\epsilon_{zz} - \epsilon_{xx}} \hat{\mathbf{x}} + \hat{\mathbf{z}} \right) e^{ik_e y}. \quad (7)$$

The corresponding magnetic field is given by  $\mathbf{H} = -i/(\omega\mu_0) \hat{\mathbf{y}} \times \partial_y \mathbf{E}$  (with  $\partial_y \equiv \partial/\partial y$ ). After some algebra, one may show that the time-averaged Poynting vector  $\mathbf{S} = \frac{1}{2} \text{Re}\{\mathbf{E} \times \mathbf{H}^*\}$  in the material is

$$\mathbf{S} = \frac{1}{2} \frac{\sqrt{\epsilon_0}}{\sqrt{\mu_0}} \left[ |A_o|^2 \sqrt{\epsilon_{xx}} + |A_e|^2 \sqrt{\epsilon_{zz}} \left( 1 + \left| \frac{\epsilon_{xz}}{\epsilon_{zz} - \epsilon_{xx}} \right|^2 \right) \right. \\ \left. + \frac{1}{\sqrt{\epsilon_{zz}} - \sqrt{\epsilon_{xx}}} \text{Re}\{\epsilon_{xz} A_e A_o^* e^{i(k_e - k_o)y}\} \right] \hat{\mathbf{y}}. \quad (8)$$

The first two terms of this expression represent the power transported by the ordinary and the extraordinary waves alone, respectively. Remarkably, provided the cross-coupling coefficient  $\epsilon_{xz}$  does not vanish, there is a third term that is responsible for a periodic spatial variation of the power flux. This third term describes a *power beating* with spatial frequency  $k_e - k_o$  as illustrated with a numerical example in Fig. 2. Thus, when  $\epsilon_{xz} \neq 0$ , the two modes cease to transport the power independently in the material. This is a rather unique result, as for any Hermitian system the electromagnetic modes always transport power independently. In fact, if the crossed term of the Poynting vector

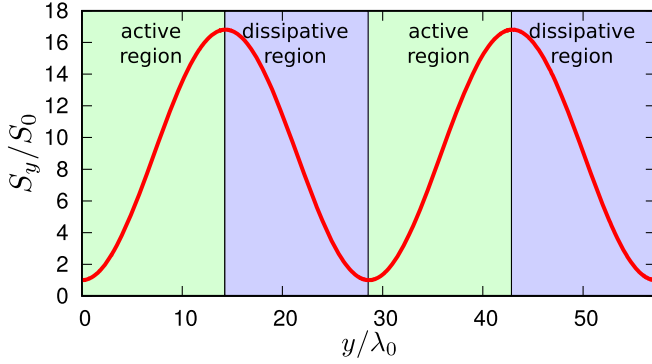


FIG. 2. Normalized Poynting vector as a function of the propagation distance  $y$  normalized to the vacuum wavelength  $\lambda_0 = 2\pi c/\omega$ . The parameters are  $\epsilon_{xx} = 2$ ,  $\epsilon_{zz} = 2.1$ ,  $\epsilon_{xz} = 0.2$ ,  $A_e = 1$  and  $A_o = -A_e[\epsilon_{xz}/(\epsilon_{zz} - \epsilon_{xx})]$ . The regions shaded in green correspond to active regions, whereas the regions shaded in purple correspond to dissipative regions.

does not vanish, the power flux forcibly depends on the propagation distance (as in Fig. 2). This is only possible in nonenergy conserving (non-Hermitian) systems, e.g., systems with loss or gain ( $\bar{\epsilon} \neq \bar{\epsilon}^\dagger$ ).

Curiously, the interplay of the static bias field with the material nonlinearity may lead to either dissipation or gain. Thus, our metamaterial may behave as either “lossy” or “gainy,” depending on the relative phase between the two propagating modes. In different words, the material is neither a standard lossy material nor a standard gainy material, but rather exhibits a dual-type response. In particular, depending on the relative phase between the ordinary and extraordinary waves, the MOSFET-metamaterial alternates between active and dissipative regions (see the Supplementary Material [92]). For the particular model considered here, the energy exchange between the wave and the medium is controlled by a polarization current induced by the static electric field through the nonlinearity [92]. The power amplification is proportional to the magnitude of the cross-coupling coefficient and can be made rather large if the values of  $\epsilon_{xx}$  and  $\epsilon_{zz}$  are sufficiently close. Similar power beatings may occur in other non-Hermitian platforms (e.g., [54]).

Next, we present a design of an electromagnetic isolator. The proposed system is depicted in Fig. 3(a) and is based on the non-orthogonality of the two eigenvectors of the bulk material. It consists of a MOSFET-metamaterial slab of thickness  $d$  placed in between two orthogonal linear polarizers. The linear polarizers are supposed to fully absorb the electric field component parallel to some axis and let the orthogonal component pass through them unchanged.

We introduce the transmission matrix  $\bar{T}$  that relates (in the absence of the polarizing grids) the transverse components of the incident  $\mathbf{E}_t^{\text{inc}} = (E_x^{\text{inc}} E_z^{\text{inc}})^T$  and transmitted  $\mathbf{E}_t^{\text{tr}} = (E_x^{\text{tr}} E_z^{\text{tr}})^T$  electric fields as  $\mathbf{E}_t^{\text{tr}} = \bar{T} \cdot \mathbf{E}_t^{\text{inc}}$ . In the supplementary information [92], it is shown that for normal

incidence ( $\mathbf{k} = k\hat{y}$  with  $k = \omega/c$ ) the transmission matrix for a material slab with thickness  $d$  is

$$\bar{T} = \begin{pmatrix} \gamma_o & \frac{\epsilon_{xz}}{\epsilon_{xx} - \epsilon_{zz}}(\gamma_o - \gamma_e) \\ 0 & \gamma_e \end{pmatrix}, \quad (9)$$

where  $\gamma_j = [\cos(k_j d) - i(k_j^2 + k^2)/(2k_j k) \sin(k_j d)]^{-1}$  with  $j = o, e$ . The transmission matrix lacks transpose symmetry and is independent of the direction of propagation of the incoming wave. The matrix has a single nonzero antidiagonal element, and hence the slab can generate an outgoing wave with  $E_x$  component from an incoming wave polarized along  $z$ , but not the converse.

Let us now analyze the response of the proposed isolator. For an incident wave propagating from left to right the polarizing grid WPG1 ensures that the field that reaches the metamaterial is oriented along the  $z$  direction with an amplitude  $E_z^{\text{inc}}$ . Because of the cross-coupling term  $\epsilon_{xz}$ , the propagation in the metamaterial may induce an electric field component along the  $x$  direction. This  $x$  component of the field can go through the grid WPG2, generating the left-to-right output signal. In contrast, an incident wave propagating from right-to-left can enter into the MOSFET-metamaterial only if the incident electric field has a component along  $x$ . In this case, the metamaterial does not generate any cross-polarization component, and thereby the incoming wave is fully absorbed at the output polarizing grid. Therefore, the wave propagation is allowed only in a specific (left-to-right) direction. This is confirmed by Eq. (9) that reveals that the right-to-left transmission coefficient  $T_{\text{iso}}^{r \rightarrow l} = T_{21}$  of the isolator is exactly zero. The left-to-right transmission  $|T_{\text{iso}}^{l \rightarrow r}| = T_{12}$  is depicted in Fig. 3(b) as a function of the isolator thickness  $d$  for different material parameters. As seen, a longer propagation distance typically yields a stronger output signal, up to some threshold value beyond which an oscillatory behavior is observed. By neglecting the reflections at the air-metamaterial interfaces, one finds that [92]

$$|T_{\text{iso}}^{l \rightarrow r}| \approx \left| 2 \frac{\epsilon_{xz}}{\epsilon_{zz} - \epsilon_{xx}} \sin\left(\frac{k_e - k_o}{2} d\right) \right|. \quad (10)$$

Hence, the transmission is maximized when  $(k_e - k_o)d = \pi$ , i.e., for a thickness  $d = d_{\text{max}} \equiv \lambda_0/(2[\sqrt{\epsilon_{zz}} - \sqrt{\epsilon_{xx}}])$ . The transmission maximum is  $|2 \tan(\theta)|$  and is controlled by the angle  $\theta$  and by the nonorthogonality of the eigenvectors [see Fig. 1(b)]. The transmission level can in principle be much greater than unity due to the active response of the metamaterial [see Fig. 3(b)(i)].

For a fixed value of  $\epsilon_{xz}$ , a larger detuning of the diagonal elements  $|\epsilon_{xx} - \epsilon_{zz}|$  leads to a decrease in  $d_{\text{max}}$ , but at the same time the transmission level drops down. This is illustrated in Fig. 3(b) where the strong amplification obtained in (i) after a propagation of around  $15\lambda_0$  becomes

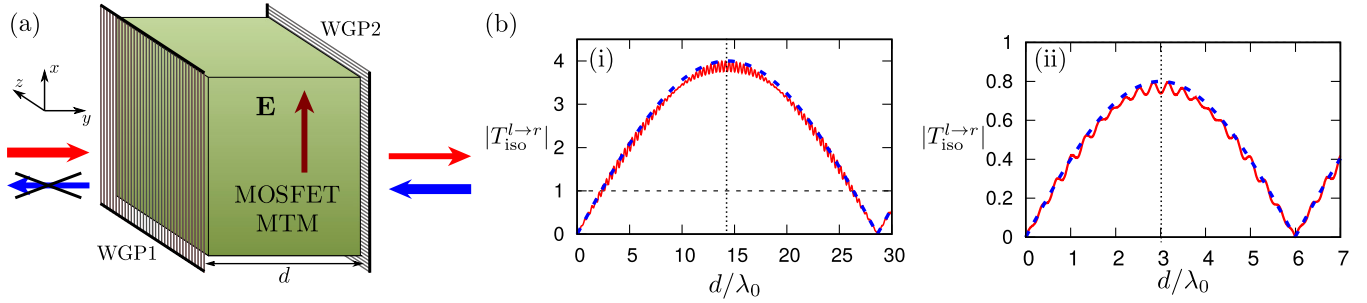


FIG. 3. (a) Electromagnetic isolator based on an electrically biased MOSFET-metamaterial placed in between two orthogonal linear polarizers. To ease the visualization the polarizers are represented as wire grids, WGP1 and WGP2, that absorb electric fields parallel to the directions of the wires, i.e., the  $x$  and  $z$  directions, respectively. The propagation from right to left is forbidden. The direction of the electric bias  $\mathbf{E}_0$  is also shown. (b) Transmission from left to right  $|T_{\text{iso}}^{l \rightarrow r}|$  as a function of the isolator thickness  $d$  normalized to the free-space wavelength. The parameters are  $\epsilon_{xx} = 2$ ,  $\epsilon_{xz} = 0.2$  and (i)  $\epsilon_{zz} = 2.1$  and (ii)  $\epsilon_{zz} = 2.5$ . The red line is the exact solution whereas the blue dashed line is the approximate solution given by Eq. (10). The vertical dotted lines mark the positions of  $d_{\text{max}}$ .

smaller than unity but the maximum is reached only after  $3\lambda_0$ .

For a device with small  $d$  Eq. (10) becomes  $|T_{\text{iso}}^{l \rightarrow r}| \approx (2\pi d/\lambda_0)|\epsilon_{xz}/(\sqrt{\epsilon_{zz}} + \sqrt{\epsilon_{xx}})|$ . Hence, for a small thickness the amplification factor is bounded by the magnitude of  $\epsilon_{xz}$ . In contrast, for a large thickness this limitation disappears, because the distributed gain is controlled by  $\epsilon_{xz}/(\epsilon_{zz} - \epsilon_{xx})$ , and thus can be arbitrarily large.

It is relevant to point out that even though the idealized metamaterial is TR invariant, the presence of the dissipative polarizing grids breaks the TR symmetry of the system [Fig. 3(a)]. In fact, it is well known that dissipation is an absolutely essential ingredient to realize an electromagnetic isolator. Moreover, our system is not affected by any of the problems that limit the performance of systems that exploit dynamic nonlinearities [77–79]. In principle our isolator can be implemented using any linearized material response with nonorthogonal eigenvectors.

In summary, we introduced a new and robust mechanism to break the Lorentz reciprocity using the combination of a static electric bias and material nonlinearities. Starting from an analogy with the operation of a semiconductor transistor, we showed that the linearization of a nonlinear material response, can lead to a nonsymmetric and non-Hermitian permittivity response. We studied in detail the wave propagation in an idealized MOSFET-metamaterial, showing that the non-Hermitian nature of the wave-matter interactions opens many exciting opportunities and can lead to a dual material behavior, where regimes of absorption alternate with regimes of gain in the same physical system. Furthermore, we suggested a design of an electromagnetic isolator using the proposed material, whose performance may in principle surpass that of standard Faraday isolators. We envision that related platforms can be engineered as metamaterials or, alternatively, can be implemented using naturally available materials in nonequilibrium situations. The prospects are especially promising up to THz frequencies, both in metamaterial [93] and in

natural material realizations. Note that the nonlinear response of naturally available materials remains strong and fast enough up to the longitudinal optical phonon resonance [94].

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